3A, 36V, 1.5MHz Synchronous Step-Down Converter

General Description

The EML3290 is frequency adjustable, 3A, step-down converter with an integrated high-side and low-side switch. The current mode control is adopted in EML3290 for fast loop response and easy compensation. The EML3290 operates with the wide input voltage from 4.5V to 36V and provides an adjustable output voltage from 0.808V to 30V. The EML3290 features a PWM mode operation with up to 1.5MHz adjustable switching frequency.

Cycle-by-cycle current limiting, output over-voltage protection and thermal shutdown are provided for fault condition protections. An internal 2ms soft-start design reduces input start-up current and prevents the output voltage and inductor current to overshooting during power-up.

The EML3290 is available in E-SOP-8L with thermally enhanced package.

Features

- 4.5V to 36V Input Voltage Range
- 3A Continuous Output Current
- 100mΩ/75 mΩ Internal Power MOSFET Switch
- Output Adjustable from 0.808V
- Up to 1.5MHz Adjustable Switching Frequency
- Cycle-by-Cycle Current Limit, Input Under-voltage Lockout, Output over-Voltage Protection and Thermal Shutdown
- Stable with Low ESR Output Ceramic Capacitors
- 2ms Internal Soft-Start
- Thermally Enhanced E-SOP-8L Package

Applications

- 12V and 24V Distributed Power Systems
- Battery Powered Systems
- Industrial Power Systems
- LCD and Plasma TVs
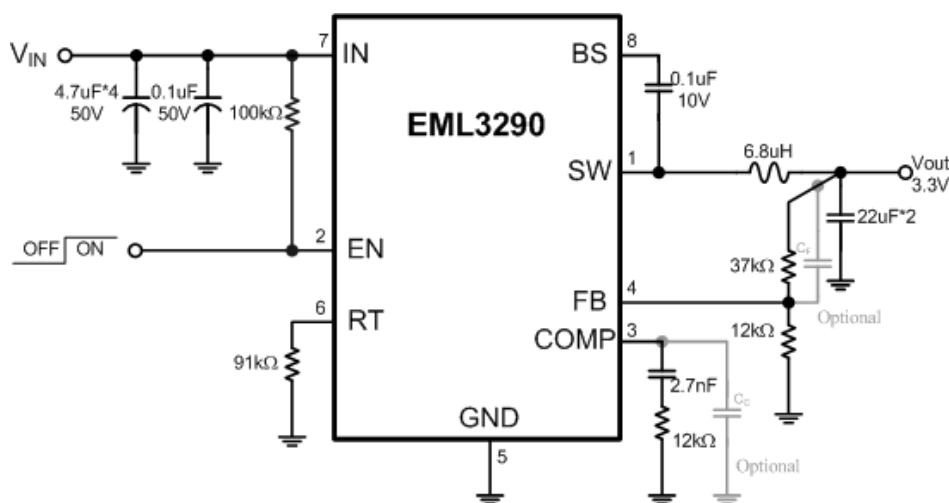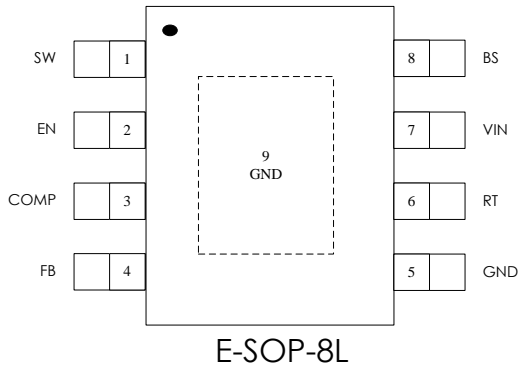- Automotive Systems

Typical Application

Fig.1

Package Configuration

E-SOP-8L

EML3290-00SG08NRR

00	Adjustable
SG08	E-SOP-8L Package
NRR	RoHS & Halogen free package
	Commercial Grade Temperature
	Rating: -40 to 85°C
	Package in Tape & Reel

Order, Mark & Packing information

Package	Vout(V)	Product ID	Marking	Packing
E-SOP-8L	Adjustable	EML3290-00SG08NRR	ESMT EML3290 Tracking code	Tape & Reel 3K units

Functional Block Diagram
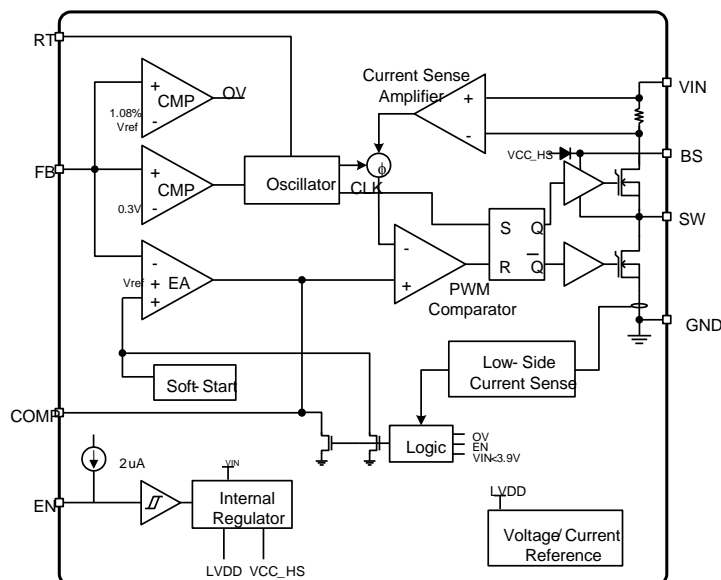
Fig.2

Pin Functions

Pin Name	E-SOP-8L	Function
SW	1	**Switch Node.** Must be connected to inductor. This pin connects to the internal main and synchronous power MOSFET switches.
EN	2	**Enable Pin.** On/Off control Input.
COMP	3	**Compensation.** This node is the output of Error Amplifier. Control loop frequency compensation is applied to this pin.
FB	4	**Feedback Pin.** This pin can be connected a resistor divider to set the output voltage range.
GND	5	**Ground Pin.** Connect exposed pad to GND plane for optimal thermal performance.
RT	6	**Frequency setting pin.** This pin can be connected to a resistor to GND to set the oscillator frequency.
VIN	7	**Supply Voltage.** The EML3290 operates from a 4.5V to 36V.
BS	8	**Bootstrap.** This is the positive power supply for the internal floating high-side MOSFET driver. Connect a bypass capacitor (0.1uF) between BS and SW pin.
GND	9	**Ground Pin/Thermal Pad** This pin must be connected to ground. The thermal pad with large thermal land area on the PCB will helpful chip power dissipation.

Absolute Maximum Ratings

Devices are subjected to fail if they stay above absolute maximum ratings.

Input Voltage(VIN) ------------------------------ – 0.3V to +42V
Switch Voltage (SW) -------------------- – 0.3V to Vin+0.3V
Boost Voltage (BS)------------------------ V_{SW}-0.3V to V_{SW}+6V
Enable Voltage (EN) ---------------------------- – 0.3V to Vin
All Other Pins (RT, FB, COMP) ------------------ – 0.3V to +6V
Lead Temperature (Soldering, 10 sec)---------------- 260°C

Ambient Operating Temperature Range –40°C to 85°C
Junction Temperature (Notes 1) --------- –40°C to 150°C
Storage Temperature Range ------------- – 65°C to 150°C
ESD Susceptibility HBM ---------------------------------- 2KV
MM ------------------------------------ 200V

Recommended Operating Conditions

Input Voltage (VIN) ----------------------------- +4.5V to +36V

Junction Operating Temperature Range –40°C to 125°C

Thermal data

Package	Thermal resistance	Parameter	Value
E-SOP-8L	θ_{JA} (Note 2)	Junction-to-ambient	50°C/W
	$\theta_{JC\,(top)}$ (Note 3)	Junction-case (top)	39°C/W
	$\theta_{JC(bottom)}$ (Note 4)	Junction-case (bottom)	10°C/W

Electrical Characteristics

VIN=12V, T_A=+25°C, unless otherwise specified.

Symbol	Parameter	Conditions	Min	Typ	Max	Units
V_{FB}	Feedback Voltage	$4.5V \leqq V_{IN} \leqq 36V$	0.788	0.808	0.828	V
$R_{ONH)}$	High-Side Switch on Resistance			100		mΩ
R_{ONL}	Low-Side Switch on Resistance			75		mΩ
I_{SW}	Switch Leakage	V_{EN}=0V, V_{SW}=0V or 12V			10	μA
I_{LIMH}	High-Side Switch Current Limit			5		A
I_{LIML}	Low-Side Switch Current Limit	From Drain to Source		1.8		A
G_{CS}	COMP to Current Sensing Transconductance (note5)			4.2		A/V
A_{EA}	Error Amplifier Voltage Gain (note5)			800		V/V
G_{EA}	Error Amplifier Transconductance (note5)	I_{COMP}=±10uA		1		mA/V
	Error Amplifier Source Current	FB=0.6V		0.1		mA
	Error Amplifier Sink Current	FB=1V		-0.1		mA
V_{UVLO}	VIN UVLO Threshold		3.9	4.2	4.5	V
	VIN UVLO Hysteresis			300		mV
V_{OVP}	VOUT Over Voltage Protection (OVP)	Percentage of V_{FB}		108		%
	VOUT OVP Hysteresis	Percentage of V_{FB}		104		%
F_{OSC}	Oscillation Frequency	V_{FB}=0.6V; RT=100kΩ		500		kHz
	Shutdown Supply Current	V_{EN}=0		8	15	μA
	Quiescent Supply Current	V_{EN}=2V,V_{FB}=1V		0.8	1.2	mA
T_{SD}	Thermal Shutdown			160		℃
	Thermal Shutdown Hysteresis			30		℃

Symbol	Parameter	Conditions	Min	Typ	Max	Units
T_{OFF}	Minimum Off Time (note5)			100		ns
T_{ON}	Minimum On Time (note5)			120		ns
	EN Input Low Voltage				0.4	V
	EN Input High Voltage		1.5			V

Note 1: T_J is a function of the ambient temperature T_A and power dissipation P_D ($T_J = T_A + (P_D)$ *θ_{JA})).

Note 2: θ_{JA} is simulated in the natural convection at T_A=25℃ on a highly effective thermal conductivity (thermal land area completed with >3x3cm^2 area) board (2 layers , 2S0P) according to the JEDEC 51-7 thermal measurement standard.

Note 3: θ_{JT} represents the heat resistance between the chip junction and the top surface of package.

Note 4: θ_{JC} represents the heat resistance between the chip junction and the center of the exposed pad on the underside of the package.
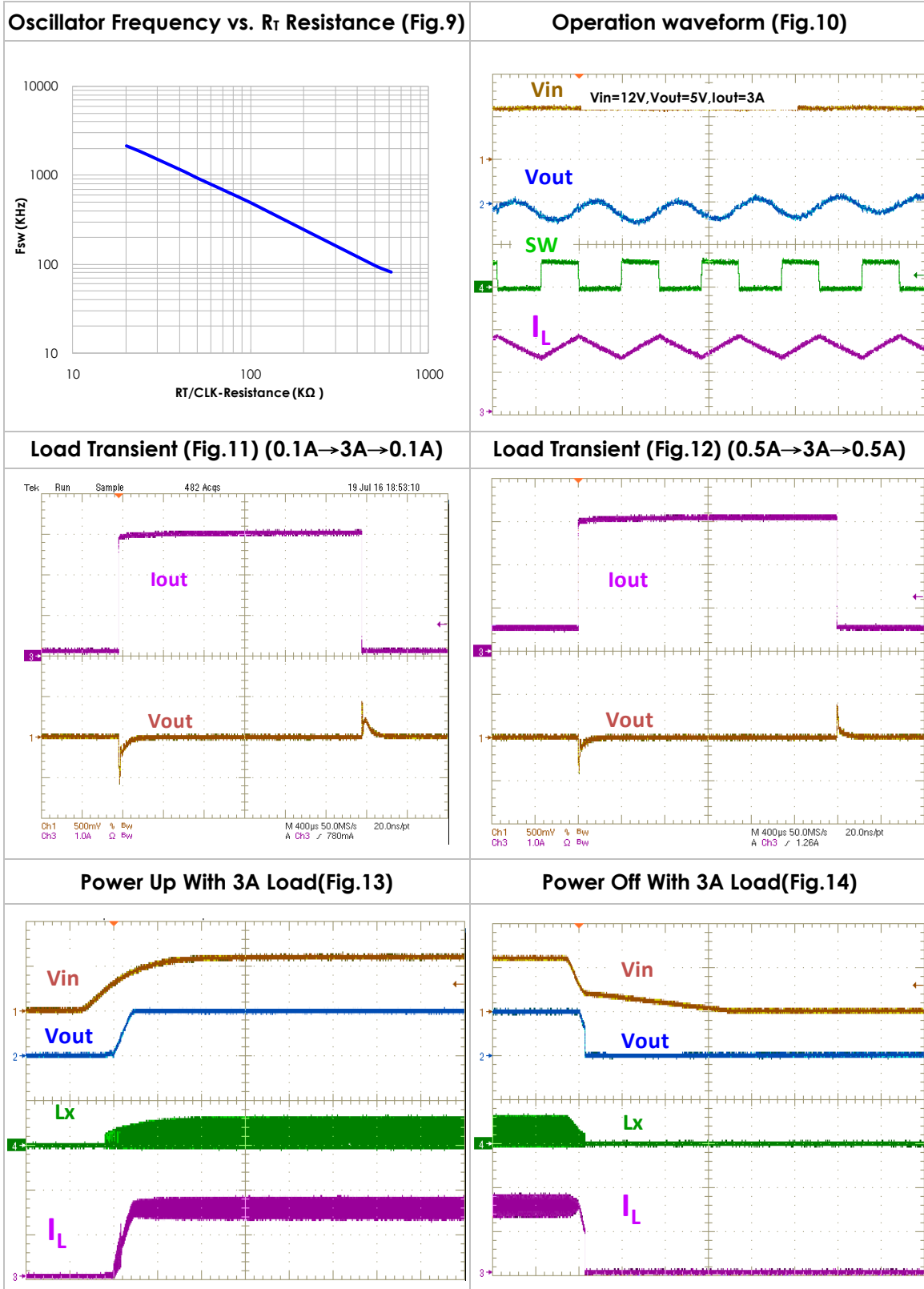
Note 5: Guaranteed by design.

Typical Performance Characteristics
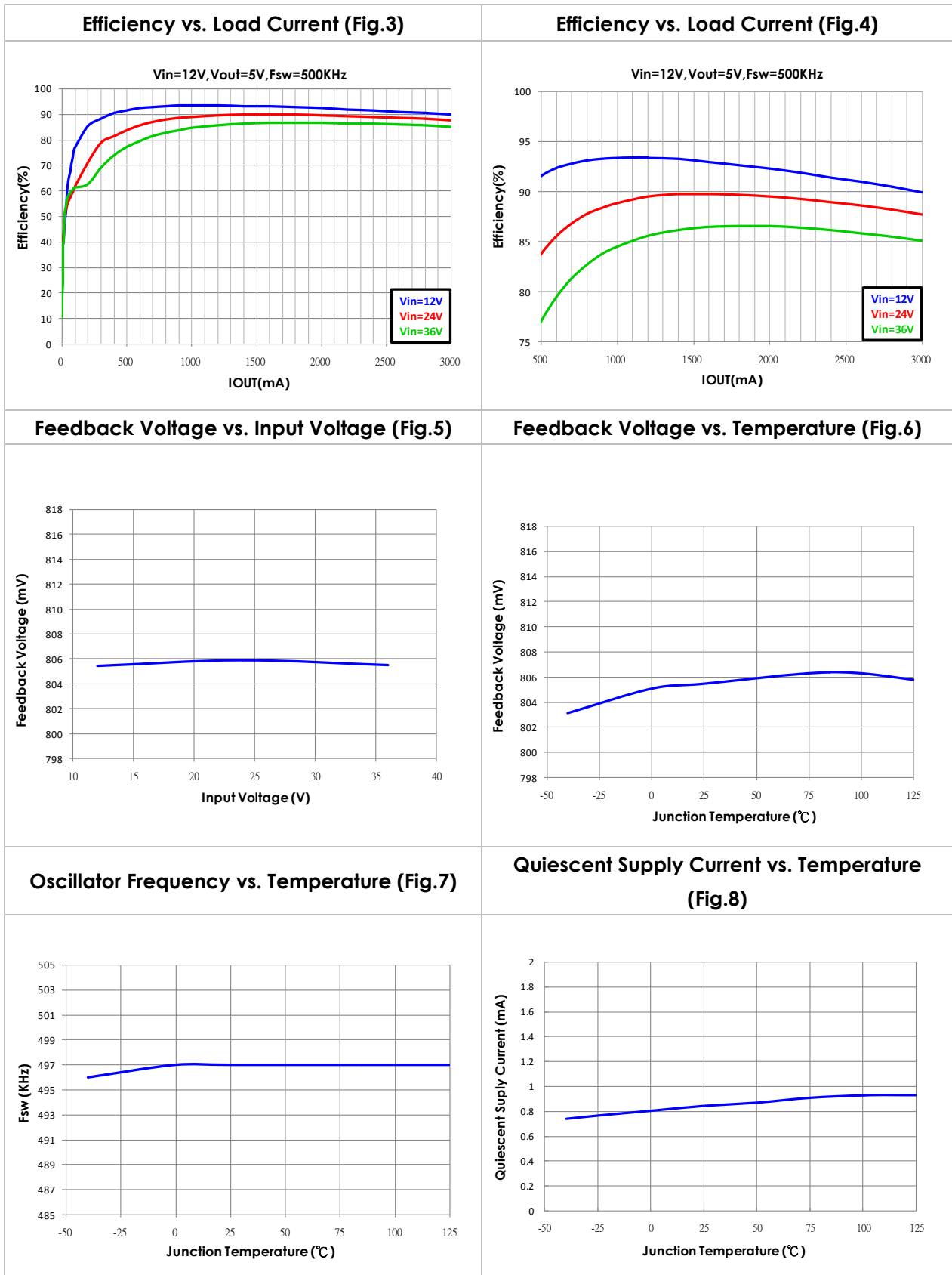
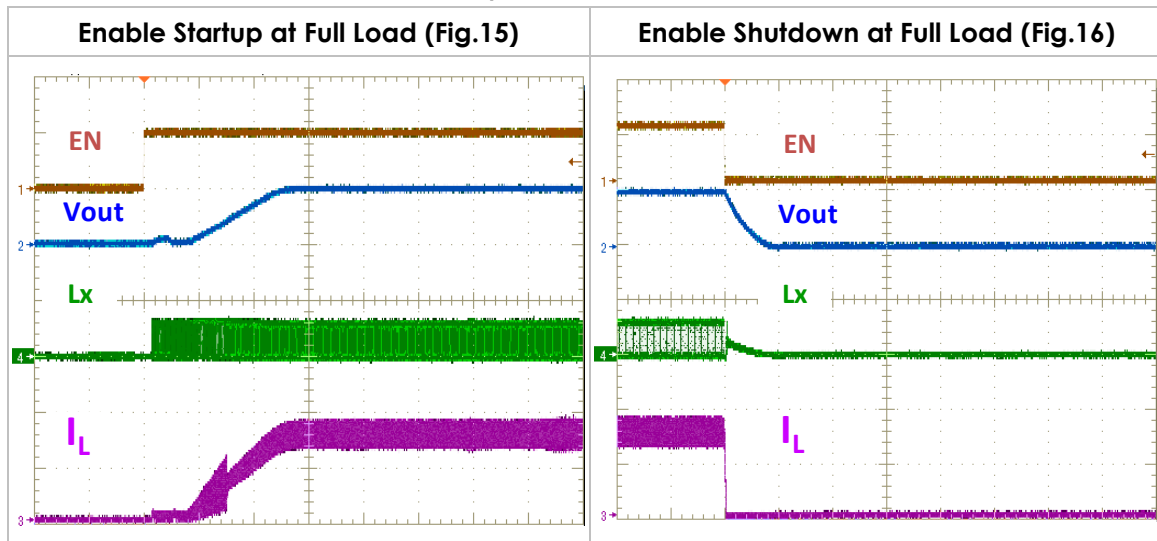V_{IN}=12V, V_{OUT}=5.0V, T_A=25℃, unless otherwise specified.

Efficiency vs. Load Current (Fig.3)

Vin=12V,Vout=5V,Fsw=500KHz

Vin=12V
Vin=24V
Vin=36V

Efficiency vs. Load Current (Fig.4)

Vin=12V,Vout=5V,Fsw=500KHz

Vin=12V
Vin=24V
Vin=36V

Feedback Voltage vs. Input Voltage (Fig.5)

Feedback Voltage vs. Temperature (Fig.6)

Oscillator Frequency vs. Temperature (Fig.7)

Quiescent Supply Current vs. Temperature (Fig.8)

Typical Performance Characteristics

V_{IN}=12V, V_{OUT}=5.0V, T_A=25℃, unless otherwise specified.

Oscillator Frequency vs. R_T Resistance (Fig.9)	Operation waveform (Fig.10)

Load Transient (Fig.11) (0.1A→3A→0.1A)	Load Transient (Fig.12) (0.5A→3A→0.5A)

Power Up With 3A Load(Fig.13)	Power Off With 3A Load(Fig.14)

Typical Performance Characteristics

V_{IN}=12V, V_{OUT}=5.0V, T_A=25℃, unless otherwise specified.

Enable Startup at Full Load (Fig.15)	Enable Shutdown at Full Load (Fig.16)

Detailed Description

The EML3290 is a variable frequency, current mode, automotive buck converter with an integrated high-side switch. The device operates with input voltages from 4.5V to 36V and tolerates input transients up to 42V. During light-load conditions, the device enters Pulse Skip Mode, automatically.

Wide Input Voltage Range (4.5V to 36V)

The EML3290 includes two separate supply inputs, VIN and BS, specified for a wide 4.5V to 36V input voltage range. VIN provides power to the device and BS provides power to the internal high-side switch driver. With respect to PWM minimum duty limit in EML3290, the safe operating voltage area shall be considering in here. The Safe Operating Voltage Area (SOVA) is showed in the fig.15.
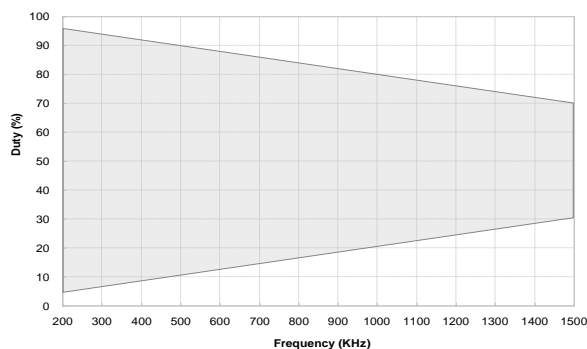
Fig.15 EML3290 Safe Operating Voltage Area

Error Amplifier

The error amplifier compares the FB pin voltage with the internal 0.80V reference and outputs a current proportional to the difference between the two. This output current is then used to charge or discharge the external compensation network on COMP pin to form the COMP voltage, which is used to control the power MOSFET current.

Minimum On-Time

The device features a 120ns minimum on-time that ensures proper operation at high switching frequency and high differential voltage between the input and the output.

Enable Control

The EML3290 has a dedicated enable control pin, EN. By pulling it high or low, that can be enabled and disabled. Tie EN to IN through a 100kΩ resistor for automatic start up. To disable the part, EN must be pulled low for at least 5us. When floating, EN is pulled up to about 2.0V by an internal 1uA current source so it is enabled. To pull it down, >10uA current capability is needed.

Over-Temperature Protection

Thermal overload protection limits the total power dissipation in the device. When the junction temperature exceeds 160℃, an internal thermal sensor shuts down the whole chip. The thermal sensor turns on the IC again after the junction temperature is cooled by 30℃

Output Over-Voltage Protection

In the case of the output voltage is stable supply in a while. Once the FB pin voltage of EML3290 is over 0.87V (~1.08xV_{FB}) from stable regulative voltage, the low-side switch would be turned on internally to discharge output over-voltage. When FB over-voltage can't be discharged below 0.84V (always above 0.84V) within 16/fs, the discharge action can be stopped.

Input Under Voltage Lock-out (UVLO)

UVLO is implemented to protect the chip from operating at insufficient supply voltage. The UVLO rising threshold is about 4.2V while its falling threshold is about 3.9V. If a higher UVLO is required for a specified application, as the EN pin shown in Fig.16 below to adjust input voltage UVLO via two external resistors and a filter capacitor. For example, choosing R3=560k and R4=62k, the V_{start} and V_{stop} would be around 10V and 7V. The EN enable threshold is around 1.0V, and with 100mV hysteresis window for shutdown.
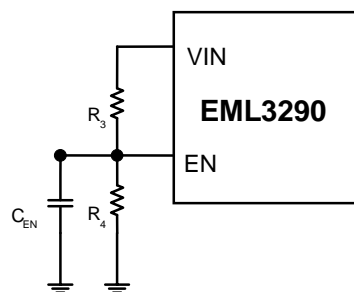

Fig.16 Two external resistors on EN pin

Boost Capacitor

Connect a 0.1uF capacitor between the BS pin and SW pin. This capacitor provides the gate driver voltage for the high-side MOSFET. Also, an UVLO in the floating supply is implemented to protect the high-side MOSFET and its driver from operating at insufficient supply voltage. The UVLO rising threshold is about 2.1V while its hysteresis is about 0.15V.

Over-Current protection

Over-current limiting is implemented by sensing the current across the high-side MOSFET. If the current exceeds the over-current threshold limit, the over-current indicator is set true. Once over-current indicator is set true, over-current limiting is triggered. The

high-side MOSFET is turned off for the rest of the cycle. The output voltage will start to drop if the output is dead-short to ground, suddenly. Once the FB is lower than 0.3V, the switching frequency of EML3290 is folded back to around 1/4 fsw. However, when the over-current indicator is set true and the FB is lower than 0.3V, the short circuit protective function will be started.

Soft-Start
The typical time of soft-start is about 2ms, and overshoot of the output voltage can be reduced by the function naturally.

Programmable Oscillator
The EML3290 oscillating frequency (200kHz~1.5MHz adjustable switching frequency) is set by an external resistor, R_T from the RT pin to GND. The value of RT can be calculated from:

$$\text{Frequency}\,(\text{kHz}) = \frac{3.75 \times 10^4}{R_T^{0.95}\,(\text{k}\Omega)}$$

Application Information

The schematic on the front page shows a typical application circuit. The IC can provide up to 3A output current at a 3.3V output voltage. For proper thermal performances, the exposed pad of the device must be soldered down to the PCB.

Setting the Output Voltage

The output voltage is set by the resistive voltage divider from the output voltage to FB pin. The voltage divider divides the output voltage down to the feedback voltage by the ratio

$$V_{FB} = Vout \times \frac{R2}{R1+R2} \Rightarrow Vout = V_{FB} \times \frac{R1+R2}{R2}$$

Table1-Resistor Selection for Common Output Voltages

Vout	R1 (kΩ)	R2 (kΩ)
1.8V	33.1 (1%)	27 (1%)
2.5V	50.2 (1%)	24 (1%)
3.3V	37 (1%)	12 (1%)
5.0V	62.3 (1%)	12 (1%)
12V	277 (1%)	20 (1%)

Selecting the Inductor

The common rule for determining the inductance to use is to allow the peak-to-peak ripple current in the inductor to be between 20% and 40% of the DC maximum load current, typical 30%. And also have sufficiently high saturation current rating and a DCR as low as possible. Generally, it is desirable to have lower inductance in switching power supplies, because it usually corresponding to faster transient response, smaller DCR and reduced size for more compact designs. But too low of an inductance results in higher ripple current such that over-current protection at full load could be falsely triggered. Also, the output ripple voltage and efficiency become worse with lower inductance. Under light load condition, like below 100mA, larger inductance is recommended for improved efficiency. The inductance and its peak current could be calculated by:

$$L = \frac{V_{OUT}}{f_S \times \Delta I_L} \cdot \left(1 - \frac{V_{OUT}}{V_{IN}}\right)$$

$$I_{LP} = I_{LOAD} + \frac{\Delta I_L}{2} = I_{LOAD} + \frac{V_{OUT}}{2 \times f_S \times L} \cdot \left(1 - \frac{V_{OUT}}{V_{IN}}\right)$$

Which f_S is the switching frequency; I_{LOAD} is the load current.

Table2-Inductor Selection Guide

Model	ISAT (A)	DCR (mΩ)	Manufacture
PCM104T-100MS	8.5	27 (typ.)	CYNTEC

Selecting the Input capacitor

The input current to the step-down converter is discontinuous, therefore a capacitor is required to supply the AC current for step-down converter to maintain the DC input voltage. Use low ESR capacitor for the best performance. The high frequency impedance of the capacitor should be lower than the input source impedance for bypassing the high frequency switching current locally. Ceramic capacitors with X5R or X7R dielectrics are highly recommended because of their low ESR and small temperature coefficients. To prevent excessive voltage ripple at input, the relationship between the input ripple and the capacitance could be estimated by:

$$\Delta V_{IN} = \frac{I_{LOAD}}{f_S \times C_{IN}} \times \frac{V_{OUT}}{V_{IN}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)$$

For 3A output applications, four 4.7uF ceramic capacitors are sufficient. For VIN<6V application, the recommended C_{IN} would be 22uF*4.

Selecting the Output capacitor

The output capacitor (C_O) is required to maintain the DC output voltage, keeps the output ripple small, and ensures regulation loop stability. The lower ESR capacitors are preferred to keep lower output ripple. The output voltage ripple can be estimated by:

$$\Delta V_{OUT} = \frac{V_{OUT}}{f_S \times L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \times \left(R_{ESR} + \frac{1}{8 \times f_S \times C_O}\right)$$

Which L is the inductance and R_{ESR} is the equivalent series resistance (ESR) of the output capacitor.

In case of lower ESR capacitor adopted, the output ripple is mainly caused by the capacitance and the output voltage ripple can be estimated by:

$$\Delta V_{OUT} = \frac{V_{OUT}}{8 \times f_S{}^2 \times L \times C_O} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)$$

Or, the ESR dominates the impedance at switching frequency. After simplification, the output voltage ripple can approximated to

$$\Delta V_{OUT} = \frac{V_{OUT}}{f_S \times L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \times R_{ESR}$$

The characteristics of the output capacitor also affect the loop stability of regulation system. Low ESR ceramic capacitors with X5R or X7R dielectrics are recommended.

Compensation Components

The EML3290 employs current mode control for easy compensation and fast transient response. The system stability and transient response are controlled through the COMP pin. COMP pin is the output of the internal error amplifier. A series capacitor-resistor combination sets a pole-zero combination to control the characteristics of the control system. The DC gain of the voltage feedback loop is given by:

$$A_{VDC} = R_L \cdot G_{CS} \cdot A_{EA} \cdot \frac{V_{FB}}{V_O}$$

Where R_L is the load resistor value, G_{CS} is the current sensing transconductance and A_{EA} is the error amplifier gain. The system has two important poles. One is due to the compensation capacitor (C_{CMP}) and the output resistor (r_O) of error amplifier, and the other is due to the output capacitor (C_O) and the load resistor (R_L). These poles are located at:

$$f_{p1} = \frac{1}{2\pi \cdot C_{CMP} \cdot r_O} = \frac{G_{EA}}{2\pi \cdot C_{CMP} \cdot A_{VEA}}$$

$$f_{p2} = \frac{1}{2\pi \cdot C_O \cdot R_L}$$

Where, G_{EA} is the error amplifier transconductance.

The system has one important zero, due to the compensation capacitor (C_{CMP}) and the compensation resistor (R_{CMP}). The zero is located at:

$$f_{Z1} = \frac{1}{2\pi \cdot C_{CMP} \cdot R_{CMP}}$$

The system may have another important zero, if the output capacitor has a large capacitance with a high ESR value. The zero, due to the ESR and a capacitance of the output capacitor, is located at:

$$f_{ESR} = \frac{1}{2\pi \cdot C_O \cdot R_{ESR}}$$

In this case, a third pole set by the compensation capacitor (C_C) which is directly connected to COMP Pin between GND and the compensation resistor (R_{CMP}) is used to compensate the effect of the ESR zero(f_{ESR}) on the loop gain. This pole is located at:

$$f_{p3} = \frac{1}{2\pi \cdot C_C \cdot R_{CMP}}$$

To shape the converter transfer function for getting an adequate loop gain is the purpose of compensation design. The system open loop unity gain crossover frequency is important.

Lower crossover frequencies result in slower line and load transient responses, while higher crossover frequencies could system unstable. A good compromise is to set the crossover frequency to below one-tenth of the switching frequency. To optimize the compensation components, the following procedure can be used:

1. Choose the compensation resistor (R_{CMP}) to set the desired crossover frequency. Determine the R_{CMP} value by the following equation:

$$R_{CMP} = \frac{2\pi \cdot C_O \cdot f_C}{G_{EA} \cdot G_{CS}} \cdot \frac{V_O}{V_{FB}}$$

Where, f_C is the desired crossover frequency.

2. Choose the compensation capacitor (C_{CMP}) to get the desired phase margin. For applications with typical inductor values, setting the compensation zero, f_{Z1}, to below one-forth of the crossover frequency provides sufficient phase margin. Determine the C_{CMP} value by the following equation:

$$C_{CMP} > \frac{4}{2\pi \cdot R_{CMP} \cdot f_C}$$

Where, R_{CMP} is the compensation resistor value.

To avoid the output voltage unstable due to the parasitic capacitor between the COMP pin and GND, the $C_{CMP}>100pF$ is strongly recommended.

3. Determine if the second compensation capacitor (C_C) is required. It is required if the ESR zero of the output capacitor is located at less than half of the switching frequency, the following relationship is valid:

$$\frac{1}{2\pi \cdot C_O \cdot R_{ESR}} < \frac{f_S}{2}$$

If this is the case, then add the second compensation capacitor C_C to set the pole f_{P3} at the location of the ESR zero. Determine the C_C value in the following equation:

$$C_C > \frac{C_O \cdot R_{ESR}}{R_{CMP}}$$

And, a 3~5pF capacitance is suggested to improve full range operating.

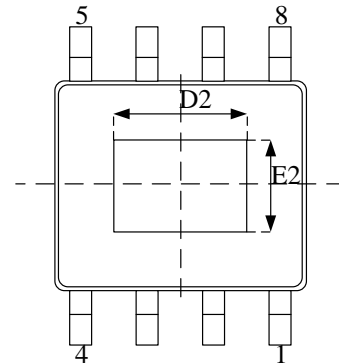**Table4-Components Selection Guide**

Vout (V)	L (uH)	C_O (uF)	R_{CMP} (kΩ)	C_{CMP} (nF)	C_C (pF)
1.8	2.2	22*2	8.2	2.7	3~5
2.5	3.6~6.8	22*2	10	2.7	3~5
3.3	4.7~10	22*2	12	2.7	3~5
5.0	6.8~10	22*2	16	2.7	3~5
12	10~22	22*2	24	2.7	3~5

4. The estimation is based on 15% of Iout current for this table. User can calculate it depend on peak-to-peak ripple current real requirement.

Package Outline Drawing

E-SOP-8L (150 mil)
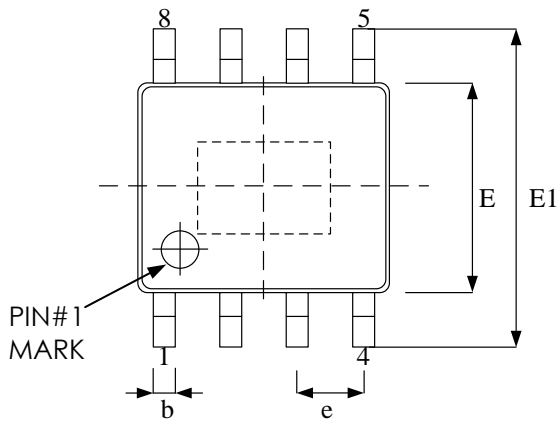
TOP VIEW

BOTTOM VIEW
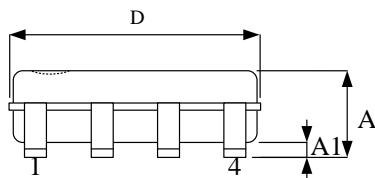
SIDE VIEW
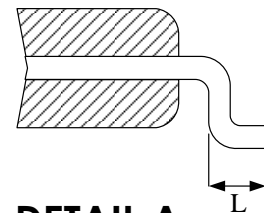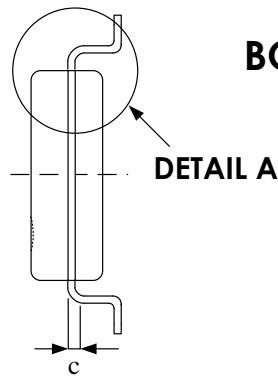
DETAIL A

DETAIL A

Symbol	Dimension in mm	
	Min	Max
A	1.35	1.75
A1	0.00	0.25
b	0.33	0.51
c	0.17	0.25
D	4.80	5.00
E	3.81	4.00
E1	5.79	6.20
e	1.27 BSC	
L	0.41	1.27

Exposed pad

	Dimension in mm	
	Min	Max
D2	1.93	2.39
E2	1.93	2.39

Revision History

Revision	Date	Description
0.01	2016.08.16	Draft version
0.02	2016.11.28	Update typical performance characteristics

Important Notice